

BNSDOCID: <WO 0055977A1 I.>

FOR THE PURPOSES OF INFORMATION ONLY

Codes used to identify States party to the PCT on the front pages of pamphlets publishing international applications under the PCT.

AL	Albania	ES	Spain	LS	Lesotho	SI	Slovenia
AM	Armenia	FI	Finland	LT	Lithuania	SK	Slovakia
AT	Austria	FR	France	LU	Luxembourg	SN	Senegal
AU	Australia	GA	Gabon	LV	Latvia	SZ	Swaziland
AZ	Azerbaijan	GB	United Kingdom	MC	Monaco	TD	Chad
BA	Bosnia and Herzegovina	GE	Georgia	MD	Republic of Moldova	TG	Togo
BB	Barbados	GH	Ghana	MG	Madagascar	TJ	Tajikistan
BE	Belgium	GN	Guinea	MK	The former Yugoslav Republic of Macedonia	TM	Turkmenistan
BF	Burkina Faso	GR	Greece	ML	Mali	TR	Turkey
BG	Bulgaria	HU	Hungary	MN	Mongolia	TT	Trinidad and Tobago
BJ	Benin	IE	Ireland	MR	Mauritania	UA	Ukraine
BR	Brazil	IL	Israel	MW	Malawi	UG	Uganda
BY	Belarus	IS	Iceland	MX	Mexico	US	United States of America
CA	Canada	IT	Italy	NE	Niger	UZ	Uzbekistan
CF	Central African Republic	JP	Japan	NL	Netherlands	VN	Viet Nam
CG	Congo	KE	Kenya	NO	Norway	YU	Yugoslavia
CH	Switzerland	KG	Kyrgyzstan	NZ	New Zealand	ZW	Zimbabwe
CI	Côte d'Ivoire	KP	Democratic People's Republic of Korea	PL	Poland		
CM	Cameroon	KR	Republic of Korea	PT	Portugal		
CN	China	KZ	Kazakstan	RO	Romania		
CU	Cuba	LC	Saint Lucia	RU	Russian Federation		
CZ	Czech Republic	LI	Liechtenstein	SD	Sudan		
DE	Germany	LK	Sri Lanka	SE	Sweden		
DK	Denmark	LR	Liberia	SG	Singapore		
EE	Estonia						

DESCRIPTION

RADIO RECEIVER

Technical Field

5 The present invention relates to a radio receiver (or a receiving section of a transceiver), to an integrated circuit embodying those elements of the receiver which are integratable and to a method of operating a radio receiver to reduce power consumption.

Background Art

10 In current mobile radio receivers, such as those used for operating in accordance with cellular telephone standards, for example GSM, channel selection is usually carried out using analogue filters, but increasingly digital implementation is being sought to reduce cost and improve flexibility. In principle a relatively wide part of the spectrum containing the wanted signal
15 can be selected by analogue filters, and the final channel detection then performed using DSP techniques. However, the ADC converter must operate at a sufficiently high sampling rate to allow processing of the whole of the band of interest, and the dynamic range must be sufficient for the worst case condition. This occurs where the wanted signal is weak, but the adjacent
20 channel interferers are strong. The power consumption of the ADC is a major problem in this approach, and can be prohibitive. It has been proposed that the power consumption can be reduced using Sigma-Delta converters where adjacent channels can be partly rejected using the decimation filters.

Disclosure of Invention

25 It is an object of the present invention to reduce further the power consumption of a radio receiver, especially a battery powered receiver.

 According to a first aspect of the present invention there is provided a receiver comprising at least one analogue-to-digital converter (ADC), means for determining the level of at least the prevailing adjacent channel
30 interference, and means for dynamically adjusting the resolution of the ADC to be no larger than that required to handle the prevailing interference and the wanted signal.

According to a second aspect of the present invention there is provided a receiver comprising means to frequency down convert an input signal to an intermediate signal, digital channel selection filtering means including at least one analogue-to-digital converter(ADC), said ADC comprising an over-sampling quantizer having a plurality of dynamically selectable quantization levels, and means responsive to the characteristics of the input signal for varying the over-sampling rate and/or matching the number of quantization levels selected to the characteristics of the input signal.

The second aspect of the present invention provides a receiver comprising means to frequency down convert an input signal to an intermediate signal, digital channel selection filtering means including at least one analogue-to-digital converter(ADC), said ADC comprising a signal combiner having first and second inputs and an output, the intermediate frequency signal being coupled to the first input, analogue filtering means coupled to said output, an over-sampling quantizer coupled to an output of the analogue filtering means, the over-sampling quantizer having an output which is coupled to digital filtering means which provides an output signal, a digital to analogue converter having an input coupled to the output of the over-sampling quantizer and an output coupled to the second input of the signal combiner which produces the difference between the signals on its first and second inputs as an output, wherein the over-sampling quantizer has a plurality of dynamically selectable quantization levels, and means responsive to the characteristics of the input signal are provided for varying the over-sampling rate and/or matching the number of quantization levels selected to the characteristics of the input signal.

In an embodiment of the present invention the intermediate frequency may be a zero IF or a low IF corresponding to say half the channel bandwidth.

According to a third aspect of the present invention there is provided a method of operating a receiver having at least one analogue to digital converter(ADC), comprising determining the level of prevailing interference and dynamically adjusting the resolution of the ADC to be no larger than that required to handle the prevailing interference and the wanted signal.

According to a fourth aspect of the present invention there is provided an integrated circuit comprising at least one analogue-to-digital converter(ADC), said ADC comprising an over-sampling quantizer having a plurality of dynamically selectable quantization levels, and means responsive
5 to the characteristics of an input signal to the ADC for varying the over-sampling rate and/or matching the number of quantization levels selected to the characteristics of the input signal.

The present invention is based on the principle that the average power consumption of the ADC can be reduced by dynamically adjusting the
10 resolution of the ADC such that it is no larger than is required to handle the prevailing interference and recover the wanted signal after processing. Typically, adjacent channels are of similar amplitude to the wanted signal. In such a case the required resolution may be small, for example 8 bits. In the worst case a much larger dynamic range may be needed, for example 14 bits,
15 leading to an increase in the power consumption.

The ADC may comprise a Sigma-Delta ADC.

US Patent Specification 5,550,544 discloses a first order Delta-Sigma ADC in which an input signal is compared with each of a plurality of preset
(n-1) reference levels and is quantized into one of n-digital output signals.
20 Thus when the amplitude of an input signal is small, the amplitude of a difference signal between the input signal entered into the quantizer and an output signal therefrom, that is the quantization noise, is small.

By the receiver in accordance with the present invention being able to control the number of quantization levels relative to the dynamic range of an
25 input signal, fewer comparisons have to be made in the case of smaller amplitude signals thus saving current compared to the solution taught in US Patent Specification 5,550,544.

In an embodiment of the present invention means are provided for estimating the required characteristics, such as dynamic range. These means
30 may comprise filters before or within the ADC structure to measure directly the energies in the wanted and unwanted bands.

Brief Description of Drawings

The present invention will now be described, by way of example, with reference to the accompanying drawings, wherein:

Figure 1 is a general block schematic diagram of a quadrature receiver operating at a low IF,

5 Figure 2 is a zero IF example of a frequency (f) versus amplitude diagram illustrating the area of operation of the ADC,

Figure 3 is a block schematic diagram of a cross coupled, continuous time fourth order, low pass Sigma-Delta ADC, and

10 Figure 4 illustrates diagrammatically the quantizer having dynamically selectable quantization levels.

In the drawings, the same reference numerals have been used to indicate corresponding features.

Modes for Carrying Out the Invention

For convenience of description the present invention will be described
15 with reference to the GSM (Global System for Mobile Communications) digital cellular telephone standard.

Referring to Figure 1, the receiver (or receiver section) comprises an antenna 10 coupled to a low noise RF amplifier 14 by way of a bandpass filter 12 which selects signals in the GSM band of 925 to 960 MHz. The signal from
20 the amplifier 14 is split at a node 16 and supplied to first inputs 18, 19 of balanced mixers 20, 21. Quadrature related local oscillator signals having a frequency offset by 100kHz (or half a channel) from the centre frequency of the received signal are supplied by a signal generator 22 to second inputs 24, 25 of the mixers 20, 21. Real and imaginary low IF outputs 26, 27 of the mixers
25 20, 21, respectively, are supplied to cross-coupled, continuous time, fourth order low pass Sigma-Delta converters 32, 33 by way of bandpass filters 28, 29 and interference measuring stages 30, 32. If it is desired to apply a measure of automatic gain control this may be applied to outputs of the filters 28, 29. The input signals to the Sigma-Delta converters 32, 33 are,
30 respectively, in-phase (I) and quadrature (Q) IF signals at 100 kHz. Each converter 32, 33 comprises in the present embodiment low pass filters LP1 and LP2, the outputs of which are applied to an over-sampled quantiser Q1,

Q2. An output from the respective quantiser Q1, Q2 is converted back to an analogue signal by respective digital to analogue converters (DAC) DAC1, DAC2 and is subtracted from the input signals in signal combiners SC1, SC2, respectively.

5 The described arrangement provides a noise shaping characteristic which significantly reduces the quantisation noise at the channel frequency of interest.

The quantisers Q1, Q2 have a variable resolution which can be preselected as a result of measurements of the prevailing signal
10 characteristics, for example interference, by the stages 30, 31. Outputs from the stages 30, 31 are applied to a controller 36 which controls the resolution of the quantisers Q1, Q2.

Outputs 34, 35 from the converters 32, 33 are applied to first decimation stages 38, 39 which provide anti-alias bandpass filtering and a reduction in the
15 sampling rate by, in the present embodiment, a factor of 6. The outputs from the first decimation stages 38, 39 are at 2.17 MHz. The signals from the first decimation stages 38, 39 are derotated in derotation stages 40, 41. Second decimating stages 42, 43 are coupled to the derotation stages 40, 41 respectively, and reduce the sampling rate by, in this embodiment, a factor of 8
20 to provide signals at 270.83 kHz, the bit rate of GSM. Outputs from the second decimating stages 42, 43 are supplied to an equaliser/demodulator stage 44 which provides an output 46.

The operation of the receiver shown in Figure 1 may be summarised by the incoming RF signal from the antenna 10 being converted in the balanced
25 mixers 20, 21 into in-phase (I) and quadrature (Q) components at a low IF equal to typically half the channel bandwidth or half the channel spacing. These I and Q signals are digitised using a pair of low-pass Sigma-Delta converters 32, 33 which have been cross-coupled in order to shift the noise shaping minimum from zero to the low IF in use. The bitstream output from
30 the Sigma-Delta converters 32, 33 is then decimated and derotated to provide a multi-bit digitised zero - IF output, the majority of the adjacent channel

filtering having been done in the decimation process. The multi-bit output is then demodulated as appropriate for the application.

Figure 2 shows by way of example the noise shaping characteristic 48 is disposed symmetrically about a zero IF channel 49 of interest. The noise floor NF is indicated by the horizontal broken line. The relatively high amplitude of the noise shaping characteristic 48 is to enable the converters 32, 33 to handle large amplitude adjacent channel interferers which in practice may not be present. If the converters 32, 33 are operated on the basis of always providing a high dynamic range, the power consumption of the converters 32, 33 will be high.

As shown, the adjacent channel interferers IF1 and IF2 may have a range of amplitudes which are not at the maximum. Accordingly by adjusting the noise shaping characteristic dynamically in accordance with the wanted signal or the amplitude of adjacent channel interferers (if greater), for example as shown in the chain-dot lines, power can be saved.

In Figure 1 the measurement stages 30, 31 may be configured to measure the amplitude of the wanted channel and the amplitude of the adjacent channel interferers and supply the results to the controller 36 which alters the resolution of the quantisers by varying the number of quantisation levels and/or the oversampling rate.

Figure 3 illustrates in greater detail a cross coupled, continuous time, fourth order low pass Sigma-Delta converter suitable for use in the receiver shown in Figure 1. The illustrated converter has been described and claimed in the Applicant's unpublished PCT Patent Application No. EP99/06786 claiming priority from British Patent Application No. 9821839.9, filed 8th October 1998.

Referring to Figure 3, quadrature related analogue low IF signals I and Q are applied respectively to input terminals 50, 51. Each input terminal 50, 51 is coupled to a fourth - order, time - continuous, Sigma - Delta converter 52, 54. Each converter 52, 54 comprises an anti-alias continuous time analogue loop filter consisting of four series connected transconductor - capacitor integrators 56, 58, 60, 62 and 57, 59, 61, 63. The second to fourth integrators

of each modulator are cross-coupled by gyrators 64, 66, 68. Each stage is set to resonate at a respective frequency in the IF band; the frequency being determined in accordance with the ratio g_m/C . The value of C is set by the noise requirements and conductance g_m is set to give the desired centre
5 frequency for that value of C . Cross coupling these stages has the effect of introducing a negative susceptance at each capacitor site whose value is determined by the shift in frequency required and the characteristic admittance of the gyrator. The first stages 56, 57 are not cross-coupled which avoids introducing a dc offset to the outputs of these stages. Outputs of each of the
10 four stages 56, 58, 60, 62 and 57, 59, 61, 63 are combined in respective summation stages 70, 72. Outputs of the stages are applied to respective quantisers Q1 and Q2 in which the analogue signals are over-sampled by $n \times F_s$, where F_s is the symbol rate, to provide digital signals having the required resolution on the outputs 36, 37, respectively. By choosing a high
15 over-sampling ratio, that is, the higher the number of samples over which the average can be made, the better will be the effective resolution of the ADC.

The outputs of the quantisers Q1, Q2 are also fed back, converted into analogue signals in DACs DAC1, DAC2 and combined in summation stages SC1, SC2 with signals on the respective input terminals 50, 51. The feedback
20 loops ensure that, in the frequency band of interest, the average value of the quantisation noise produced by the quantisers Q1, Q2 is as small as possible, to make the averaging process worthwhile.

The bit streams on the outputs 74, 75 of the Sigma-Delta converters are applied to the first decimation stages 38, 39 (Figure 1) which reduce the
25 sample rate, reduce the very high levels of noise produced by the Sigma - Delta converters outside the wanted signal bandwidth and provide the majority of the receiver's channel selectivity. The decimated signal is then de-rotated and decimated further to reduce the bit rate to that required for a GSM signal.

Figure 4 is a diagram of one of the quantisers Q1 or Q2. In order to be
30 able to vary the resolution of the quantiser in dependence on the size of the wanted signal or the interferers, the quantiser has a plurality of preset levels which can be selected by the controller 36. If a 1 bit resolution is required the

quantiser has a single level referenced "0". Other linearly spaced levels referenced 0.25; 0.50; 0.75; 1.0 and -0.25; -0.50; -0.75 and -1.0 can be selected to give improved resolution.

One method of varying the resolution is to pair off the corresponding complementary levels such as 0.25 and -0.25 and to dynamically select more and more pairs as the need for increased resolution rises and vice versa. In Figure 4, the selection of each of the pairs is controlled by a respective switch B1 to E1 in conjunction with the operation of a multi-position switch 80. For say 2-bit resolution, switch B1 is closed so that when the switch 80 is at position B there are three levels of quantisation 0, 0.25 and -0.25. For the next higher resolution switches B1 and C1 are closed and the switch 80 is at position C and so on until for the highest resolution all the switches B1 to E1 are closed. In practice the quantiser is implemented as a plurality of gates and comparators. Thus when a low resolution is required many gates and comparators are de-energised thus saving current.

Optionally and/or additionally the over-sampling rate of the quantisers Q1, Q2 may be varied. When altering the resolution and/or over-sampling of the quantisers Q1, Q2 concomitant changes may have to be effected to other parts, for example filters, used in the receiver shown in Figure 1 or the Sigma-Delta converters shown in Figure 3.

If desired the receiver shown in Figure 1 may be adapted to operate the quadrature related stages at zero IF by altering the local oscillator frequency to equal the notional carrier frequency of the signals on the first inputs 18, 19 of the balanced mixers 20, 21.

In a non-illustrated embodiment of the present invention the interference measuring stages 30, 31 (Figure 1) may be arranged within the Sigma-Delta converter.

In the present specification and claims the word "a" or "an" preceding an element does not exclude the presence of a plurality of such elements. Further, the word "comprising" does not exclude the presence of other elements or steps than those listed.

From reading the present disclosure, other modifications will be apparent to persons skilled in the art. Such modifications may involve other features which are already known in the design, manufacture and use of radio receivers and components therefor and which may be used instead of or in addition to features already described herein.

Industrial Applicability

Radio receivers, especially for use in cellular telephone handsets, and integrated circuits therefor.

CLAIMS

1. A receiver comprising at least one analogue-to-digital converter (ADC), means for determining the level of at least the prevailing adjacent channel interference, and means for dynamically adjusting the resolution of the ADC to be no larger than that required to handle the prevailing interference and the wanted signal.

2. A receiver comprising means to frequency down convert an input signal to an intermediate signal, digital channel selection filtering means including at least one analogue-to-digital converter(ADC), said ADC comprising an over-sampling quantizer having a plurality of dynamically selectable quantization levels, and means responsive to the characteristics of the input signal for varying the over-sampling rate and/or matching the number of quantization levels selected to the characteristics of the input signal.

3. A receiver comprising means to frequency down convert an input signal to an intermediate signal, digital channel selection filtering means including at least one analogue-to-digital converter(ADC), said ADC comprising a signal combiner having first and second inputs and an output, the intermediate frequency signal being coupled to the first input, analogue filtering means coupled to said output, an over-sampling quantizer coupled to an output of the analogue filtering means, the over-sampling quantizer having an output which is coupled to digital filtering means which provides an output signal, a digital to analogue converter having an input coupled to the output of the over-sampling quantizer and an output coupled to the second input of the signal combiner which produces the difference between the signals on its first and second inputs as an output, wherein the over-sampling quantizer has a plurality of dynamically selectable quantization levels, and means responsive to the characteristics of the input signal are provided for varying the over-sampling rate and/or matching the number of quantization levels selected to the characteristics of the input signal.

4. A receiver as claimed in claim 1, 2 or 3, characterised in that there are provided filters for measuring characteristics of the wanted channel signal and at least the adjacent channel signals and means for selecting the over-sampling rate and/or number of quantisation levels in response to the measurements made by the filters.

5. A receiver as claimed in any one of claims 1 to 4, characterised in that the ADC is a Sigma-Delta ADC.

10

6. A method of operating a receiver having at least one analogue to digital converter(ADC), comprising determining the level of at least the prevailing adjacent channel interference and dynamically adjusting the resolution of the ADC to be no larger than that required to handle the prevailing interference and the wanted signal.

15

7. A method as claimed in claim 6, characterised in that the ADC includes a quantizer having a plurality of selectable quantization levels and the resolution is adjusted by varying the number of levels selected to match the dynamic range of the prevailing interference.

20

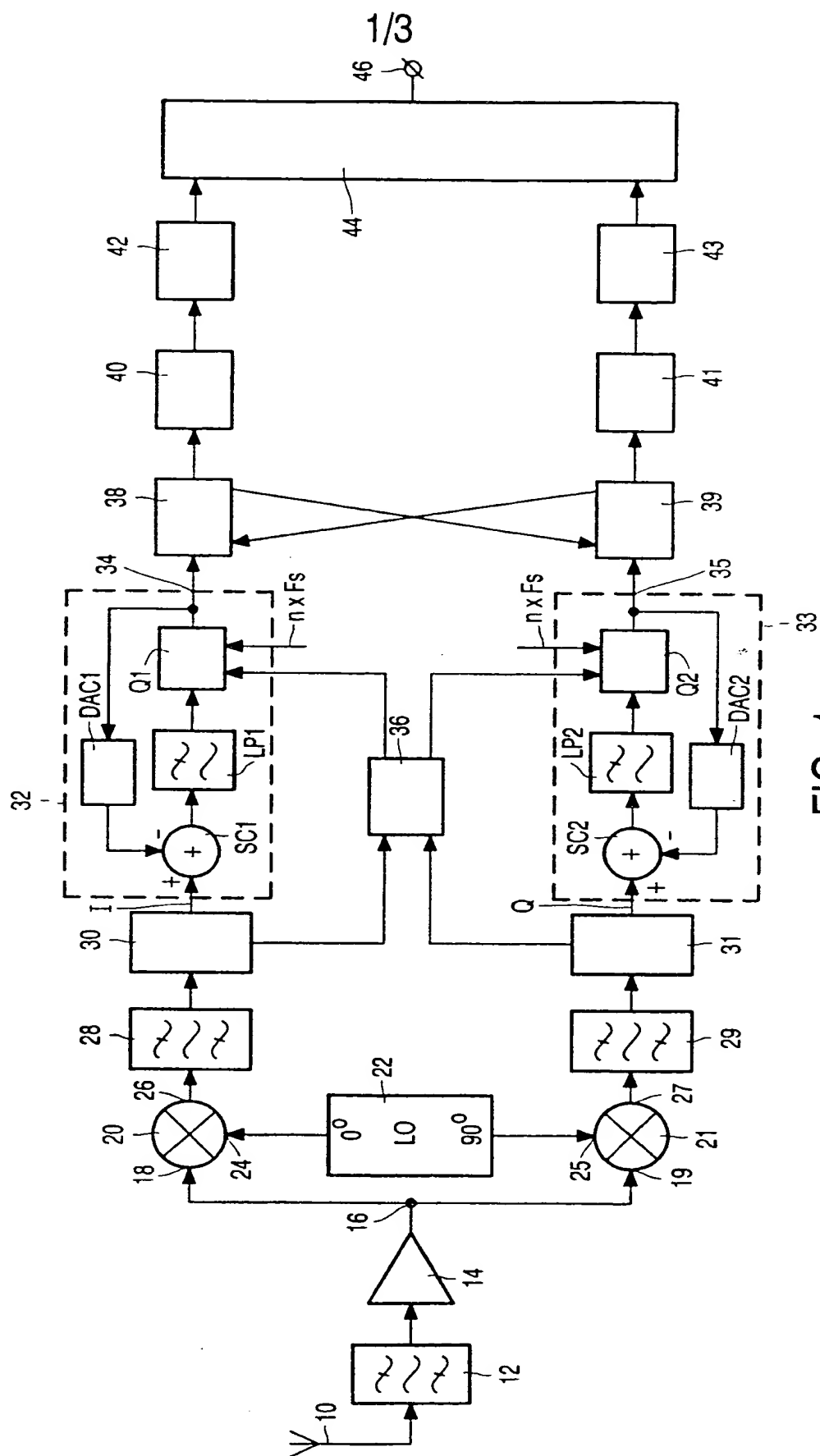
8. A method as claimed in claim 6, characterised in that the ADC includes an over-sampling quantiser and in that the rate of sampling is varied to suit the required resolution.

25

9. An integrated circuit comprising at least one analogue-to-digital converter(ADC), said ADC comprising an over-sampling quantizer having a plurality of dynamically selectable quantization levels, and means responsive to the characteristics of an input signal to the ADC for varying the over-sampling rate and/or matching the number of quantization levels selected to the characteristics of the input signal.

30

10. An integrated circuit as claimed in Claim 9, characterised in that the ADC is a Sigma-Delta ADC.



2/3

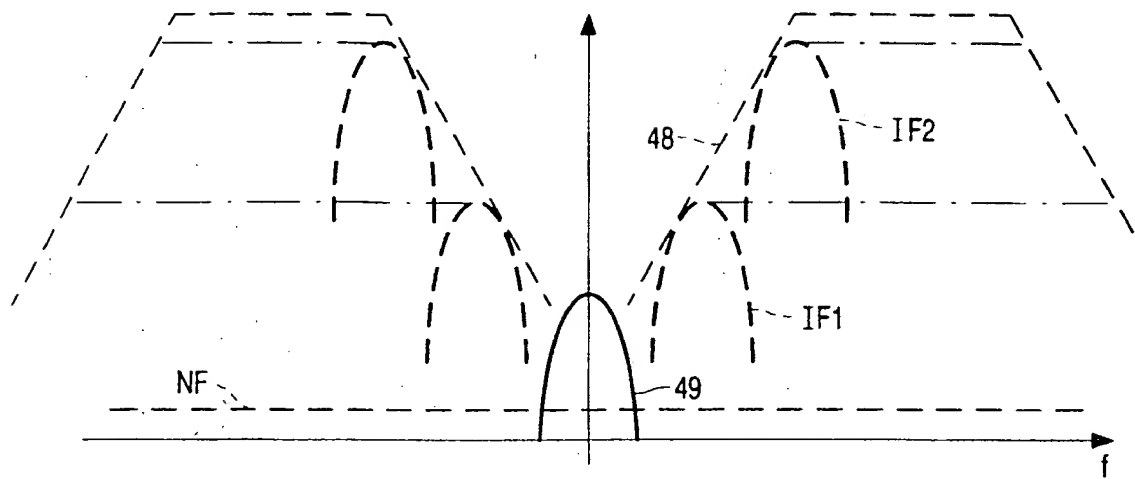


FIG. 2

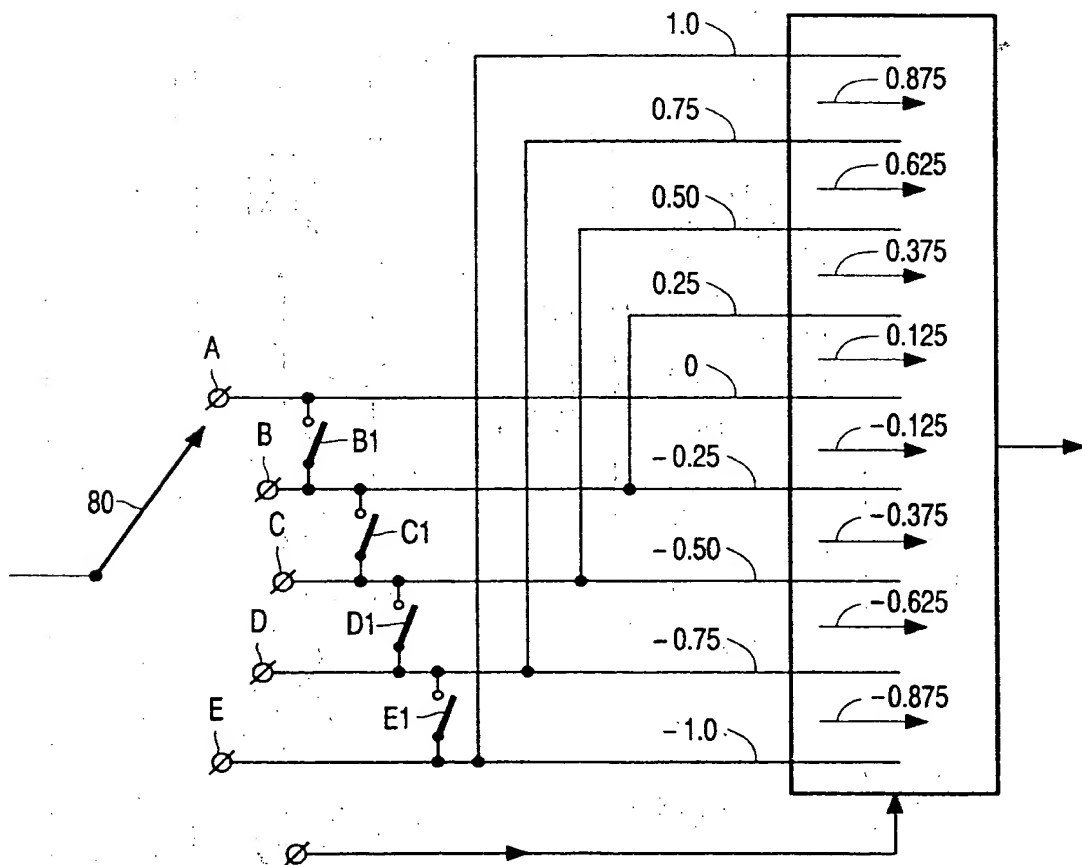


FIG. 4

3/3

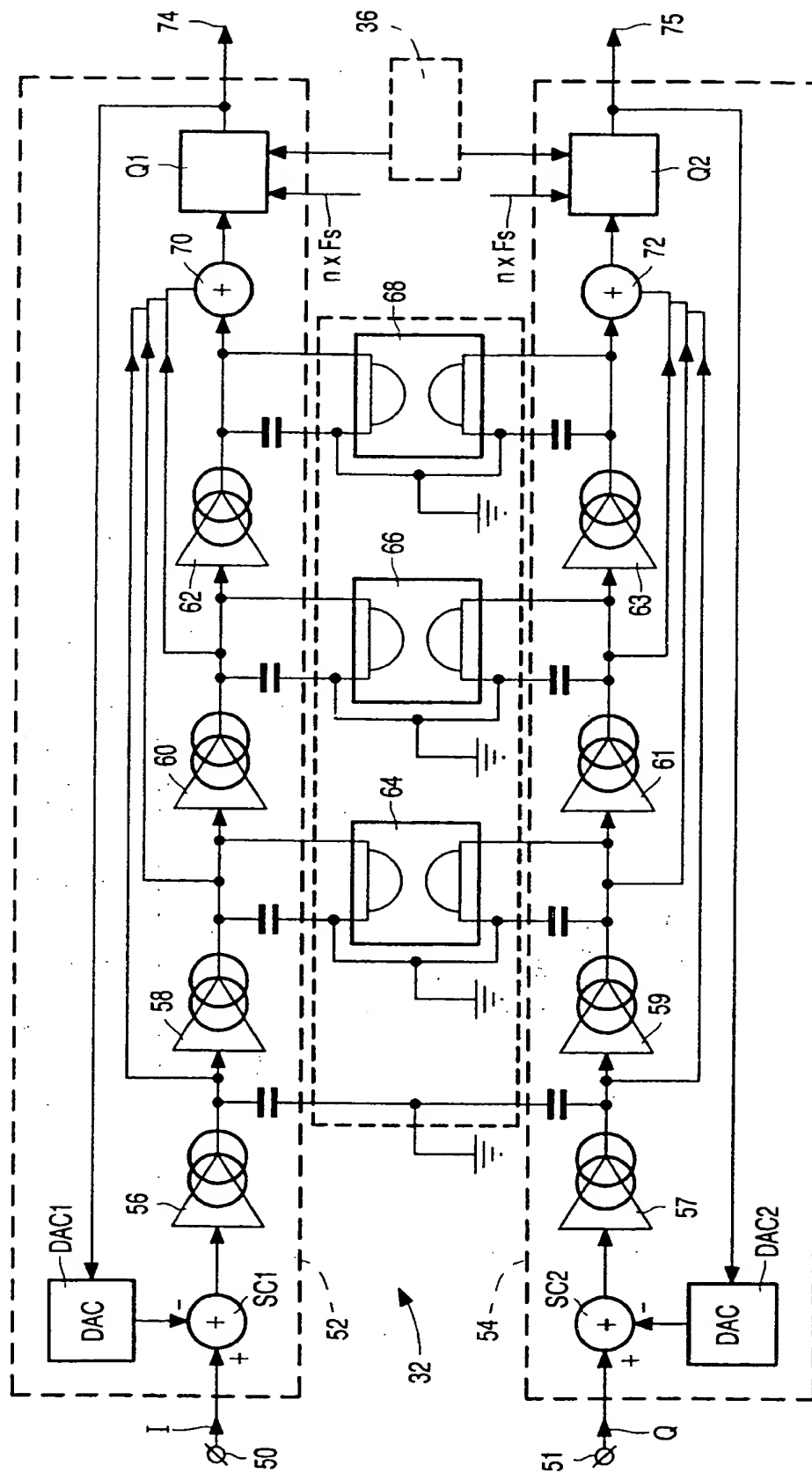


FIG. 3

INTERNATIONAL SEARCH REPORT

Inter. Appl. No.
PCT/EP 00/01342

A. CLASSIFICATION OF SUBJECT MATTER
IPC 7 H04B1/16 H04B1/10

According to International Patent Classification (IPC) or to both national classification and IPC

B. FIELDS SEARCHED

Minimum documentation searched (classification system followed by classification symbols)
IPC 7 H04B

Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched

Electronic data base consulted during the international search (name of data base and, where practical, search terms used)

C. DOCUMENTS CONSIDERED TO BE RELEVANT

Category *	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
X	US 4 910 752 A (YESTER JR FRANCIS R ET AL) 20 March 1990 (1990-03-20)	1,4-6
A	abstract column 2, line 34 -column 5, line 44 column 6, line 56 -column 7, line 2	2,3,7-10
A	US 5 625 359 A (SOBOL JAMES M ET AL) 29 April 1997 (1997-04-29) abstract column 2, line 47 -column 3, line 46; figure 2	1-10

☐ Further documents are listed in the continuation of box C.

☒ Patent family members are listed in annex.

* Special categories of cited documents:

- "A" document defining the general state of the art which is not considered to be of particular relevance
- "E" earlier document but published on or after the international filing date
- "L" document which may throw doubts on priority claim(s) or which is cited to establish the publication date of another citation or other special reason (as specified)
- "O" document referring to an oral disclosure, use, exhibition or other means
- "P" document published prior to the international filing date but later than the priority date claimed

- "T" later document published after the international filing date or priority date and not in conflict with the application but cited to understand the principle or theory underlying the invention
- "X" document of particular relevance; the claimed invention cannot be considered novel or cannot be considered to involve an inventive step when the document is taken alone
- "Y" document of particular relevance; the claimed invention cannot be considered to involve an inventive step when the document is combined with one or more other such documents, such combination being obvious to a person skilled in the art
- "&" document member of the same patent family

Date of the actual completion of the international search

31 May 2000

Date of mailing of the international search report

08/06/2000

Name and mailing address of the ISA

European Patent Office, P.B. 5818 Patentlaan 2
NL - 2280 HV Rijswijk
Tel. (+31-70) 340-2040, Tx. 31 651 epo nl,
Fax: (+31-70) 340-3016

Authorized officer

Tzimeas, K

INTERNATIONAL SEARCH REPORT

Information on patent family members

Inter national Application No

PCT/EP 00/01342

Patent document cited in search report	Publication date	Patent family member(s)	Publication date
US 4910752 A	20-03-1990	US 4811362 A	07-03-1989
		AT 111288 T	15-09-1994
		CA 1313538 A	09-02-1993
		DE 3851440 D	13-10-1994
		DE 3851440 T	30-03-1995
		DK 626689 A	12-12-1989
		EP 0394257 A	31-10-1990
		HK 1000364 A	06-03-1998
		IL 85874 A	16-09-1991
		JP 2503977 T	15-11-1990
		JP 2866094 B	08-03-1999
		KR 9615174 B	01-11-1996
		WO 8810548 A	29-12-1988
US 5625359 A	29-04-1997	US 5619202 A	08-04-1997
		DE 69510083 D	08-07-1999
		DE 69510083 T	05-01-2000
		EP 0793876 A	10-09-1997
		WO 9616482 A	30-05-1996
		US 5625358 A	29-04-1997
		US 5528240 A	18-06-1996
		US 5574454 A	12-11-1996
		US 5552785 A	03-09-1996

THIS PAGE BLANK (USPTO)